9 MHz, High Slew Rate, RRIO, CMOS Amplifiers

1 Features

- Wide Unity-Gain Bandwidth: 9MHz
- High Slew Rate: 8.5V/μs
- Fast Settling: 0.3μs to 0.1%
- Low Noise: 13nV/√Hz at 1kHz
- Low Input Offset Voltage: ±0.7mV
- Single 2.3V to 5.5V Power Supply Range
- Rail-to-Rail Input and Output
- Internal RF/EMI Filter
- Low Supply Current: 700μA at 5V Supply Per Amplifier
- Extended Temperature Range: −40°C to +125°C

2 Applications

- Motor Phase Current Sense
- Photodiode Amplification
- Audio Outputs
- Active Filters
- Driving A/D Converters
- Portable Equipment
- Battery-Powered Instrumentation

3 Description

The GD30AP863x family of single-, dual-, and quad- channel operational amplifiers represents a new generation of general-purpose, low-power op-amps. Featuring railto-rail input and output (RRIO) swings, low quiescent current (typical 700μA) combined with a wide bandwidth (9MHz) and very low noise (13nV/√Hz at 1kHz) makes this family very attractive for a variety of battery-powered applications that require a good balance between cost and performance, such as audio outputs, motor phase current sensing, photodiode amplification, barcode scanners and white goods. The low input bias current supports these amplifiers to be used in applications with mega-ohm source impedances. The robust design of the GD30AP863x amplifiers provides ease-of-use to the circuit designer: unity-gain stability with capacitive loads of up to 500pF, integrated RF/EMI rejection filter, no phase reversal in overdrive conditions, and high electro-static discharge (ESD) protection (3kV HBM). The GD30AP863x amplifiers are optimized for operation at voltages as low as +2.3V (±1.15V) and up to +5.5V (±2.75V) over the extended temperature range of −40°C to +125°C. The GD30AP8631 (single) is available in SOT23-5L package. The GD30AP8632 (dual) is offered in both SOIC-8L, DFN-8L and MSOP8L packages. The quad-channel GD30AP8634 is offered in SOIC-14L package.

Device Information[1]

PART NUMBER	PACKAGE	BODY SIZE (NOM)
GD30AP8631	SOT23-5L	2.92mm x 1.63mm
GD30AP8632	DFN2x2-8L	2.00mm x 2.00mm
	SOIC-8L	4.90mm x 3.92mm
	MSOP-8L	3.00mm x 3.00mm
GD30AP8634	SOIC-14L	8.73mm x 3.95mm

1. For all available packages, see the *Package Information* and *Ordering Information* at the end of data sheet.

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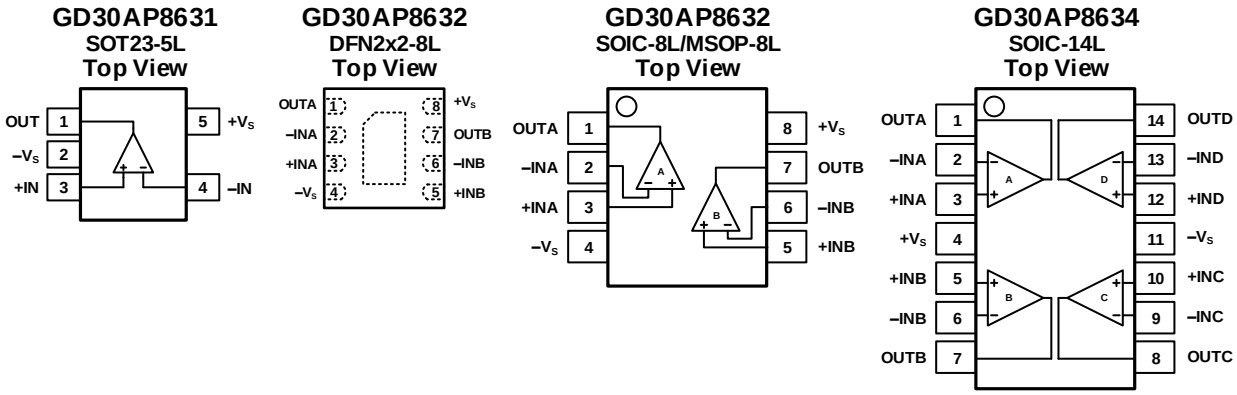
4 Device Overview

4.1 Pinout and Pin Assignment



4.2 Pin Description

NAME	PIN TYPE[1]	FUNCTION
-IN	I	Inverting input of the amplifier. The voltage range is from (V_{S-} – 0.1V) to (V_{S+} + 0.1V).
+IN	I	Non-inverting input of the amplifier. This pin has the same voltage range as –IN.
$+V_S$	P	Positive power supply. The voltage is from 2.3V to 5.5V. Split supplies are possible as long as the voltage between V_{S+} and V_{S-} is from 2.3V to 5.5V.
$-V_S$	P	Negative power supply. It is normally tied to ground. It can also be tied to a voltage other than ground as long as the voltage between V_{S+} and V_{S-} is from 2.3V to 5.5V.
OUT	O	Amplifier output.

1. I = Input, O = Output, P = Power.

5 Parameter Information

5.1 Absolute Maximum Ratings

Exceeding the operating temperature range (unless otherwise noted)[1]

SYMBOL	PARAMETER	MIN	MAX	UNIT
V_{S+} to V_{S-}	Supply Voltage		10.0	V
V_I	Signal Input Voltage	V_{S-} − 0.5	V_{S+} + 0.5	V
I_I	Signal Input Current	−10	10	mA
	Output Short-Circuit		Continuous	s
T_J	Junction Temperature, T_J		150	°C
T_{stg}	Storage Temperature Range, T_{stg}	−65	+150	°C
	Lead Temperature Range (Soldering 10 sec)		260	°C

1. The maximum ratings are the limits to which the device can be subjected without permanently damaging the device. Note that the device is not guaranteed to operate properly at the maximum ratings. Exposure to the absolute maximum rating conditions for extended periods may affect device reliability.

5.2 Recommended Operation Conditions

SYMBOL[1,2]	PARAMETER	MIN	TYP	MAX	UNIT
V_{S-} to V_{S+}	Input supply voltage range(T_A = –40°C to +125°C)	2.3		5.5	V
V_{CM}	Common-mode voltage range	V_{S-} – 0.1		V_{S+} + 0.1	V
T_A	Operating temperature range	−40		125	°C

1. The device is not guaranteed to function outside of its operating conditions.

5.3 Electrical Sensitivity

SYMBOL	CONDITIONS	VALUE	UNIT
$V_{ESD(HBM)}$	Human-body model (HBM), ANSI/ESDA/JEDEC JS-001-2017[1]	±3000	V
$V_{ESD(CDM)}$	Charge-device model (CDM), ANSI/ESDA/JEDEC JS-002-2022[2]	±2000	V

1. JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process.
2. JEDEC document JEP157 states that 250-V CDM allows safe manufacturing with a standard ESD control process.

5.4 Thermal Characteristics

SYMBOL[1]	CONDITIONS	PACKAGE	VALUE	UNIT
Θ_{JA}	Package Thermal Resistance	SOT23-5L	190	°C/W
		DFN2x2-8L	94	
		MSOP-8L	216	
		SOIC-8L	125	
		SOIC-14L	115	

1. Thermal characteristics are based on simulation, and meet JEDEC document JESD51-7.

5.5 Electrical Characteristics

V_S = 5.0 V, V_{CM} = V_S /2, V_O = V_S /2, and R_L = 10kΩ connected to V_S /2, T_A = +25°C, unless otherwise noted. Boldface limits apply over the specified temperature range, T_A = −40 to +125°C.

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNIT
OFFSET VOLTAGE						
V_{OS}	Input offset voltage			±0.7	±3.5	mV
dV_{OS}/d_T	Offset voltage drift[1]	T_A = −40 to +125°C		±2		μV/°C
PSRR	Power supply rejection ratio	V_S = 2.3 to 5.5 V, V_{CM} < V_{S+} − 2V	90	106		dB
		T_A = −40 to +125°C	77			
INPUT BIAS CURRENT						
I_B	Input bias current[1]			1		pA
		T_A = +85°C		150		
		T_A = +125°C		500		
I_{OS}	Input offset current[1]			1		pA
NOISE						
V_n	Input voltage noise	f = 0.1 to 10Hz		4.2		uV_{P-P}
e_n	Input voltage noise density	f = 1KHz		13		nV/√Hz
I_n	Input current noise density	f = 1KHz		5		fA/√Hz
INPUT VOLTAGE						
V_{CM}	Common-mode voltage range		V_{S-} − 0.1		V_{S-} + 0.1	V
CMRR	Common-mode rejection ratio	V_{CM}= −0.1 to 5.1V	70	82		dB
		V_{CM} = 0 to 4.9V, T_A= −40 to +125°C	67			
		V_S = 2.3V, V_{CM} = −0.1 to 2.1V	66	77		
		V_{CM} = 0 to 1.8V, T_A= −40 to +125°C	62			
INPUT IMPEDANCE						
C_{IN}	Input capacitance	Differential		2.0		pF
		Common mode		3.5		
OPEN-LOOP GAIN						
A_{VOL}	Open-loop voltage gain	R_L = 10kΩ, V_O = 0.05 to 3.5V	93	102		dB
		T_A = −40 to +125°C	84			
		R_L = 600Ω, V_O = 0.15 to 3.5V	78	87		
		T_A = −40 to +125°C	70			

Electrical Characteristics

V_S = 5.0 V, V_{CM} = V_S /2, V_O = V_S /2, and R_L = 10kΩ connected to V_S /2, T_A = +25°C, unless otherwise noted. Boldface limits apply over the specified temperature range, T_A = −40 to +125 °C.

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNIT
FREQUENCY RESPONSE						
GBW	Gain band width product			9		MHz
SR	Slew rate	G = +1,C_L= 100pF, V_O= 1.5 to 3.5V		8.5		V/μs
THD+N	Total harmonic distortion + noise	G = +1, f = 1KHz, V_O = 0.5V_{RMS}		0.0008		%
t_S	Settling time	To 0.1%, G = +1, 1V step		0.3		μs
		To 0.01%, G = +1, 1V step		0.4		
t_{OR}	Overload recovery time	V_{IN} * Gain > V_S		0.3		μs
OUTPUT						
V_{OH}	High output voltage swing	R_L= 10kΩ	V_{S+} − 14	V_{S+} − 10		mV
		R_L= 600Ω	V_{S+} − 200	V_{S+} − 140		
V_{OL}	Low output voltage swing	R_L= 10kΩ		V_{S-} + 7	V_{S-} + 10	mV
		R_L= 600Ω		V_{S-} + 100	V_{S-} + 150	
I_{SC}	Short-circuit current			±70		mA
POWER SUPPLY						
V_S	Operating supply voltage	T_A= −40°C to +125°C	2.3		5.5	V
I_Q	Quiescent current (per amplifier)	V_S = 2.5V		600	730	μA
		V_S = 5V		700	850	

1. Guaranteed by design and engineering sample characterization.

5.6 Typical Characteristics

V_{CM} = V_S / 2, and R_L = 10kΩ connected to V_S / 2, at T_A = +25°C, unless otherwise noted.

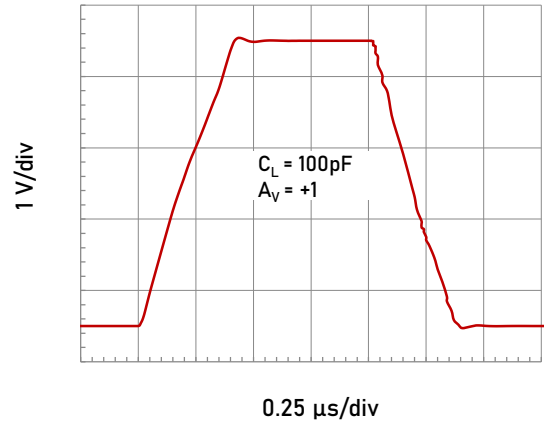


Figure 1. Large Signal Step Response

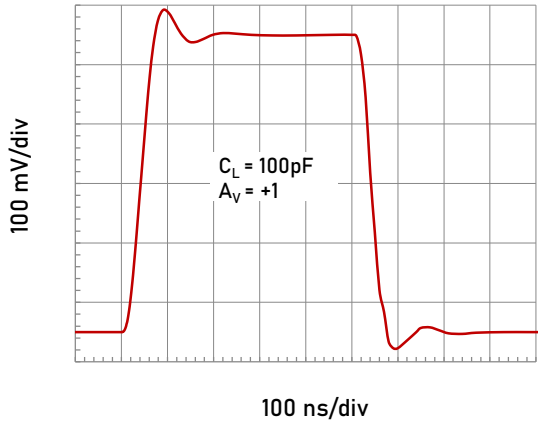


Figure 2. Small Signal Step Response (500mV)

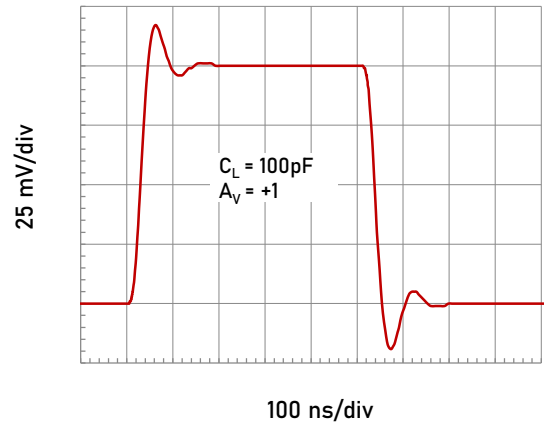


Figure 3. Small Signal Step Response (100mV)

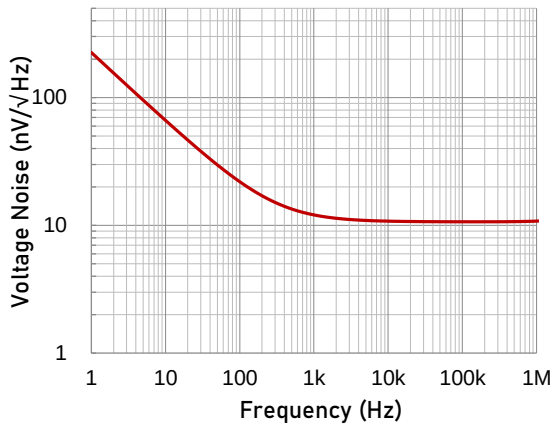


Figure 4. Input Voltage Noise Spectral Density vs. Frequency

Typical Characteristics (continued)

V_{CM} = V_S / 2, and R_L = 10kΩ connected to V_S/2, at T_A = +25°C, unless otherwise noted.

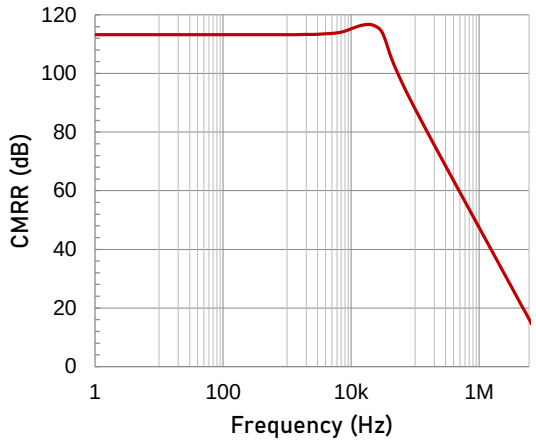


Figure 5. Common Mode Rejection Ratio vs. Frequency

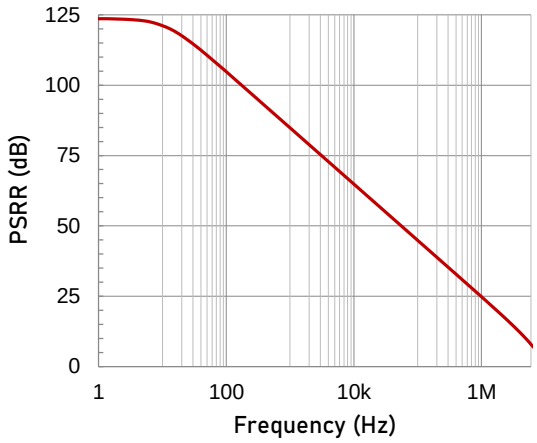


Figure 6. Power Supply Rejection Ratio vs. Frequency

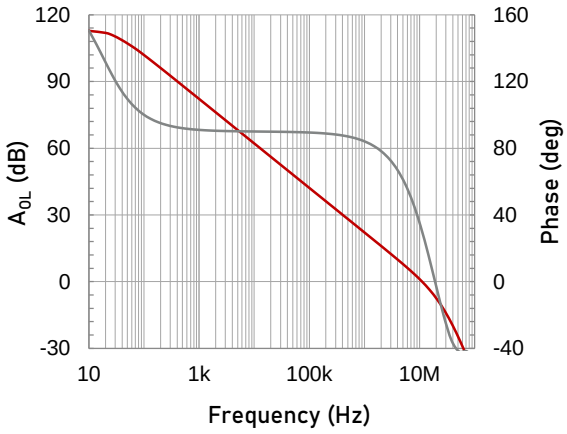


Figure 7. Open Loop Gain and Phase vs. Frequency

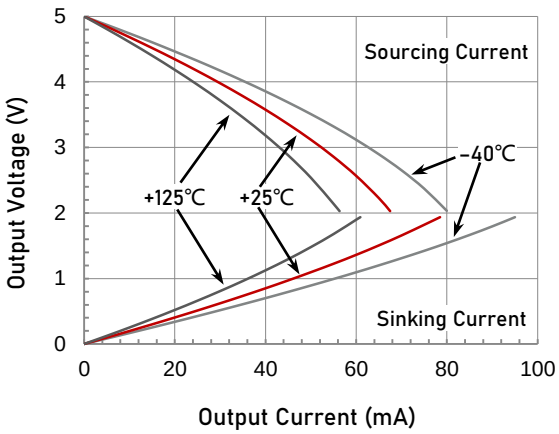


Figure 8. Output Swing vs. Output Current

Typical Characteristics (continued)

V_{CM} = V_S / 2, and R_L = 10kΩ connected to V_S/2, at T_A = +25°C, unless otherwise noted.

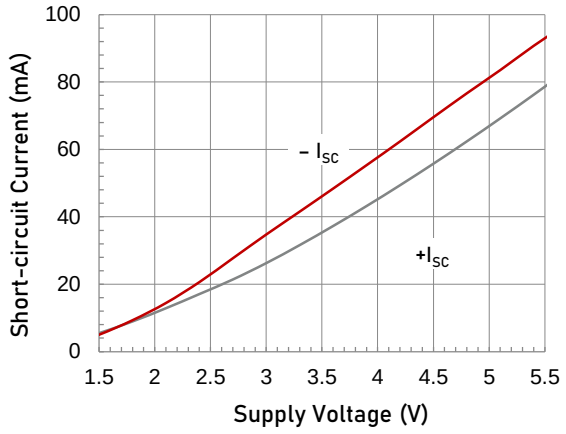


Figure 9. Short Circuit Current vs. Supply Voltage

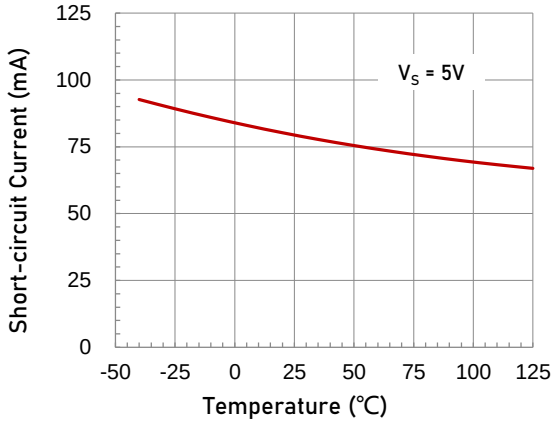


Figure 10. Short Circuit Current vs. Temperature

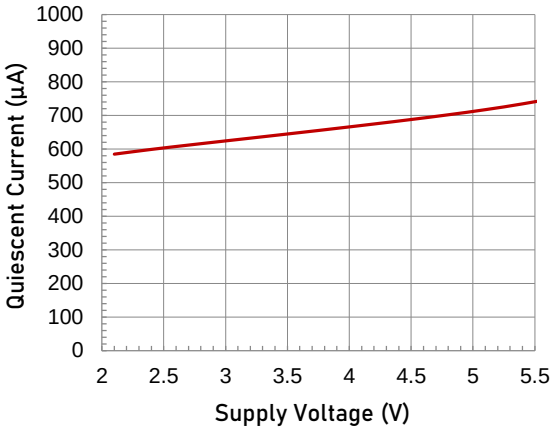


Figure 11. Quiescent Current vs. Supply Voltage

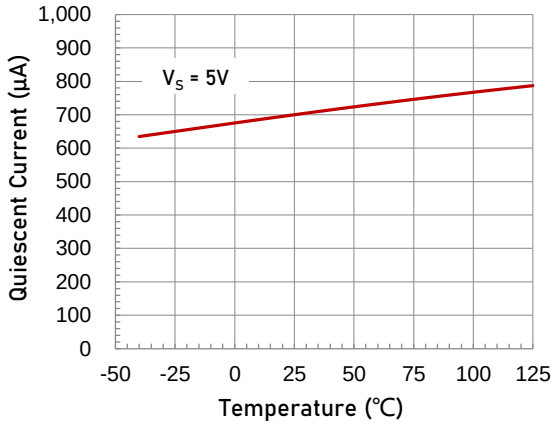


Figure 12. Quiescent Current vs. Temperature

6 Functional Description

The GD30AP863x is a family of low-power, rail-to-rail input and output operational amplifiers specifically designed for portable applications. These devices operate from 2.3V to 5.5V at the temperature range of -40°C to 125°C, are unity-gain stable, and suitable for a wide range of general-purpose applications. The class AB output stage is capable of driving ≤ 10kΩ loads connected to any point between V_{S+} and ground. The input common-mode voltage range includes both rails, and allows the GD30AP863x family to be used in virtually any single-supply application. Rail-to-rail input and output swing significantly increases dynamic range, especially in low-supply applications, and makes them ideal for driving sampling analog-to-digital converters (ADCs).

The GD30AP863x features 9MHz bandwidth and 8.5V/μs slew rate with only 700μA supply current per amplifier, providing good ac performance at very low power consumption. DC applications are also well served with a low input noise voltage of 13nV/√Hz at 1kHz, low input bias current, and an input offset voltage of 0.7mV typically. The typical offset voltage drift is 1μV/°C, over the full temperature range the input offset voltage changes only 100μV (0.7mV to 0.8mV).

6.1 Operating Voltage

The GD30AP863x family is optimized for operation at voltages as low as +2.3V (±1.15V) and up to +5.5V (±2.75V) In addition, many specifications apply from –40°C to +125°C. Parameters that vary significantly with operating voltages or temperature are illustrated in the *Typical Characteristics* graphs.

NOTE: Supply voltages (V_{S+} to $V_{S–}$) higher than +10 V can permanently damage the device.

6.2 Rail-to-Rail Input

The input common-mode voltage range of the GD30AP863x series extends 100mV beyond the negative and positive supply rails. This performance is achieved with a complementary input stage: an N-channel input differential pair in parallel with a P-channel differential pair. The N-channel pair is active for input voltages close to the positive rail, typically V_{S+}−1.4V to the positive supply, whereas the P-channel pair is active for inputs from 100mV below the negative supply to approximately V_{S+}−1.4V. There is a small transition region, typically V_{S+}−1.2V to V_{S+}−1V, in which both pairs are on. This 200mV transition region can vary up to 200mV with process variation. Thus, the transition region (both stages on) can range from V_{S+}−1.4V to V_{S+}−1.2V on the low end, up to V_{S+}−1V to V_{S+} −0.8V on the high end. Within this transition region, PSRR, CMRR, offset voltage, offset drift, and THD can be degraded compared to device operation outside this region.

The typical input bias current of the GD30AP863x during normal operation is approximately 1pA. In overdriven conditions, the bias current can increase significantly. The most common cause of an overdriven condition occurs when the operational amplifier is outside of the linear range of operation. When the output of the operational amplifier is driven to one of the supply rails, the feedback loop requirements cannot be satisfied and a differential input voltage develops across the input pins. This differential input voltage results in activation of parasitic diodes inside the front-end input chopping switches that combine with electromagnetic interference (EMI) filter resistors to create the equivalent circuit. Notice that the input bias current remains within specification in the linear region.

6.3 Input EMI Filter and Clamp Circuit

Figure 13 shows the input EMI filter and clamp circuit. The GD30AP863x op-amps have internal ESD protection diodes (D1, D2, D3, and D4) that are connected between the inputs and each supply rail. These diodes protect

the input transistors in the event of electrostatic discharge and are reverse biased during normal operation. This protection scheme allows voltages as high as approximately 500mV beyond the rails to be applied at the input of either terminal without causing permanent damage. These ESD protection current-steering diodes also provide in-circuit, input overdrive protection, as long as the current is limited to 20mA as stated in the *Absolute Maximum Ratings*.

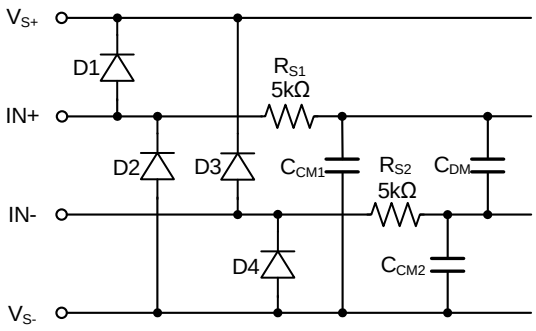


Figure 13. Input EMI Filter and Clamp Circuit

Operational amplifiers vary in susceptibility to EMI. If conducted EMI enters the operational amplifier, the dc offset at the amplifier output can shift from its nominal value when EMI is present. This shift is a result of signal rectification associated with the internal semiconductor junctions. Although all operational amplifier pin functions can be affected by EMI, the input pins are likely to be the most susceptible. The EMI filter of the GD30AP863x family is composed of two 5kΩ input series resistors (R_{S1} and R_{S2}), two common-mode capacitors (C_{CM1} and C_{CM2}), and a differential capacitor (C_{DM}). These RC networks set the −3dB low-pass cutoff frequencies at 35MHz for common-mode signals, and at 22MHz for differential signals.Package Information

6.4 Rail-to-Rail Output

Designed as a micro-power, low-noise operational amplifier, the GD30AP863x delivers a robust output drive capability. A class AB output stage with common- source transistors is used to achieve full rail-to-rail output swing capability. For resistive loads up to 100kΩ, the output swings typically to within 5mV of either supply rail regardless of the power-supply voltage applied. Different load conditions change the ability of the amplifier to swing close to the rails. For resistive loads up to 600Ω, the output swings typically to within 140mV of the positive supply rail and within 100mV of the negative supply rail.

6.5 Capacitive Load and Stability

The GD30AP863x family can safely drive capacitive loads of up to 500pF in any configuration. As with most amplifiers, driving larger capacitive loads than specified may cause excessive overshoot and ringing, or even oscillation. A heavy capacitive load reduces the phase margin and causes the amplifier frequency response to peak. Peaking corresponds to over-shooting or ringing in the time domain. Therefore, it is recommended that external compensation be used if the GD30AP863x op-amps must drive a load exceeding 500pF. This compensation is particularly important in the unity-gain configuration, which is the worst case for stability.

A quick and easy way to stabilize the op-amp for capacitive load drive is by adding a series resistor, R_{ISO}, between the amplifier output terminal and the load capacitance, as shown in Figure 14. R_{ISO} isolates the amplifier output and feedback network from the capacitive load. The bigger the R_{ISO} resistor value, the more stable V_{OUT} will be. Note that this method results in a loss of gain accuracy because R_{ISO} forms a voltage divider with the R_L.

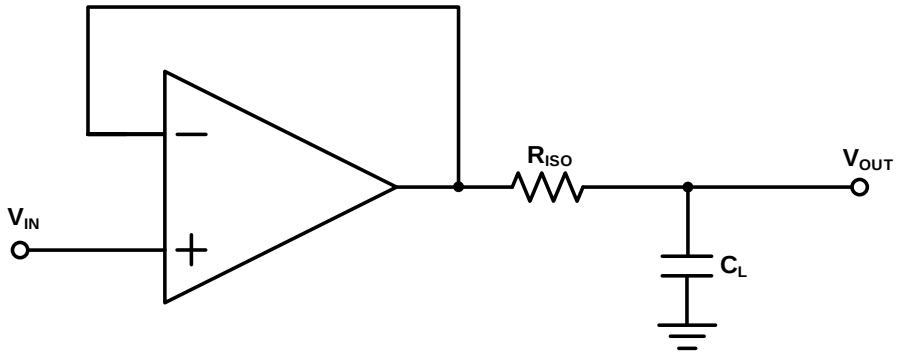


Figure 14. Indirectly Driving Heavy Capacitive Load

An improvement circuit is shown in Figure 15. It provides DC accuracy as well as AC stability. The R_F provides the DC accuracy by connecting the inverting signal with the output.

The C_F and R_{ISO} serve to counteract the loss of phase margin by feeding the high frequency component of the output signal back to the amplifier's inverting input, thereby preserving phase margin in the overall feedback loop.

For no-buffer configuration, there are two others ways to increase the phase margin: (a) by increasing the amplifier's gain, or (b) by placing a capacitor in parallel with the feedback resistor to counteract the parasitic capacitance associated with inverting node.

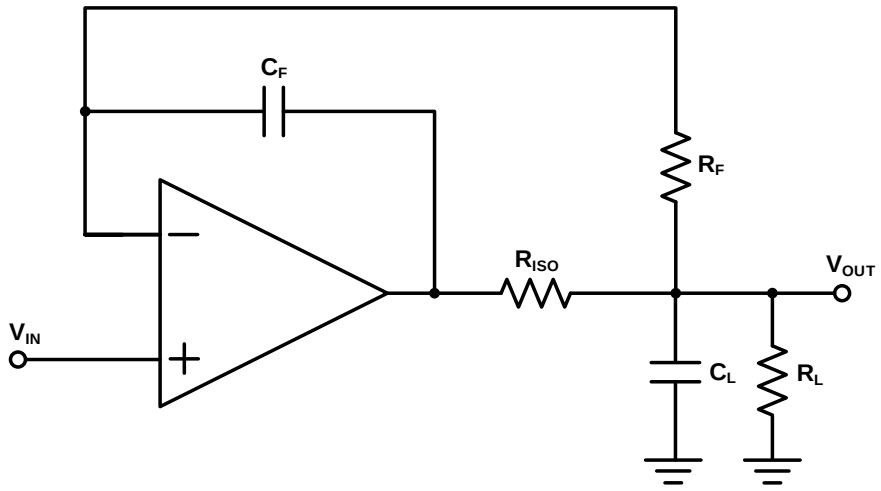


Figure 15. Indirectly Driving Heavy Capacitive Load with DC Accuracy

6.6 Overload Recovery

Overload recovery is defined as the time required for the operational amplifier output to recover from a saturated state to a linear state. The output devices of the operational amplifier enter a saturation region when the output voltage exceeds the rated operating voltage, either because of the high input voltage or the high gain. After the device enters the saturation region, the charge carriers in the output devices require time to return back to the linear state. After the charge carriers return back to the linear state, the device begins to slew at the specified slew rate. Thus, the propagation delay in case of an overload condition is the sum of the overload recovery time and the slew time. The overload recovery time for the GD30AP863x family is approximately 0.3μs.

6.7 EMI Rejection Ratio

Circuit performance is often adversely affected by high frequency EMI. When the signal strength is low and transmission lines are long, an op-amp must accurately amplify the input signals. However, all op- amp pins — the non-inverting input, inverting input, positive supply, negative supply, and output pins — are susceptible to EMI signals. These high frequency signals are coupled into an op-amp by various means, such as conduction, near field radiation, or far field radiation. For example, wires and printed circuit board (PCB) traces can act as antennas and pick up high frequency EMI signals.

Amplifiers do not amplify EMI or RF signals due to their relatively low bandwidth. However, due to the nonlinearities of the input devices, op-amps can rectify these out of band signals. When these high frequency signals are rectified, they appear as a dc offset at the output.

The GD30AP863x op-amps have integrated EMI filters at their input stage. A mathematical method of measuring EMIRR is defined as follows:

$$EMIRR = 20 \times \log\left(\frac{V_{IN\_PEAK}}{\Delta V_{OS}}\right) \quad (1)$$

6.8 Input-to-Output Coupling

To minimize capacitive coupling, the input and output signal traces should not be parallel. This helps reduce unwanted positive feedback.

6.9 Maximizing Performance Through Proper Layout

To achieve the maximum performance of the extremely high input impedance and low offset voltage of the GD30AP863x op-amps, care is needed in laying out the circuit board. The PCB surface must remain clean and free of moisture to avoid leakage currents between adjacent traces. Surface coating of the circuit board reduces surface moisture and provides a humidity barrier, reducing parasitic resistance on the board. The use of guard rings around the amplifier inputs further reduces leakage currents. Figure 16 shows proper guard ring configuration and the top view of a surface-mount layout. The guard ring does not need to be a specific width, but it should form a continuous loop around both inputs. By setting the guard ring voltage equal to the voltage at the non-inverting input, parasitic capacitance is minimized as well. For further reduction of leakage currents, components can be mounted to the PCB using Teflon standoff insulators.

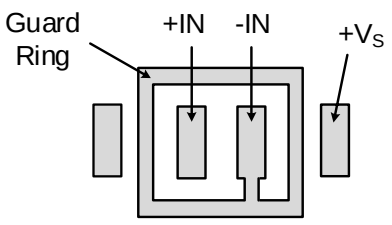


Figure 16. Use a Guard Ring around Sensitive Pins

Other potential sources of offset error are thermoelectric voltages on the circuit board. This voltage, also called Seebeck voltage, occurs at the junction of two dissimilar metals and is proportional to the temperature of the junction. The most common metallic junctions on a circuit board are solder-to-board trace and solder-to-

component lead. If the temperature of the PCB at one end of the component is different from the temperature at the other end, the resulting Seebeck voltages are not equal, resulting in a thermal voltage error.

This thermocouple error can be reduced by using dummy components to match the thermoelectric error source. Placing the dummy component as close as possible to its partner ensures both Seebeck voltages are equal, thus canceling the thermocouple error. Maintaining a constant ambient temperature on the circuit board further reduces this error. The use of a ground plane helps distribute heat throughout the board and reduces EMI noise pickup.

7 Application Information

7.1 Typical Application Circuit

7.1.1 Active Filter

The GD30AP863x family is well-suited for active filter applications that require a wide bandwidth, fast slew rate, low-noise, single-supply operational amplifier. Figure 17 shows a 500kHz, second-order, low-pass filter using the multiple-feedback (MFB) topology. The components have been selected to provide a maximally-flat Butterworth response. Beyond the cut-off frequency, roll-off is –40dB/dec. The Butterworth response is ideal for applications that require predictable gain characteristics, such as the anti-aliasing filter used in front of an ADC.

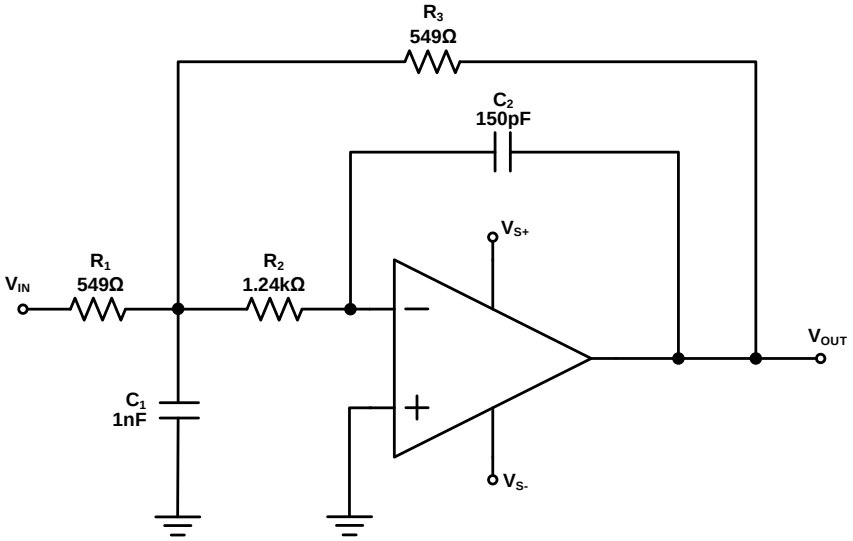


Figure 17. Second-Order, Butterworth, 500kHz Low-Pass Filter

One point to observe when considering the MFB filter is that the output is inverted, relative to the input. If this inversion is not required, or not desired, a non-inverting output can be achieved through one of these options:

1. adding an inverting amplifier;
2. adding an additional second-order MFB stage;
3. using a non-inverting filter topology, such as the Sallen-Key (shown in Figure 18).

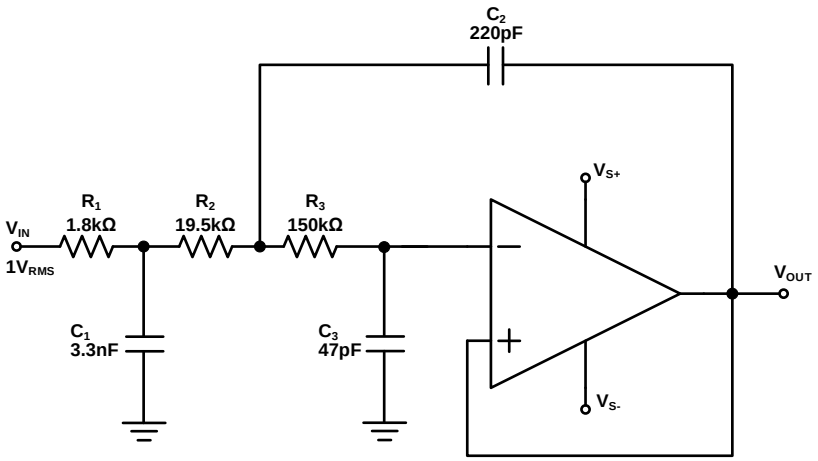


Figure 18. Configured as a Three-Pole, 20KHz, Sallen-Key Filter

7.1.2 Motor Phase Current Sensing

The current sensing amplification shown in Figure 19 has a slew rate of $2\pi fV_{PP}$ for the output of sine wave signal, and has a slew rate of $2fV_{PP}$ for the output of triangular wave signal. In most of motor control systems, the PWM frequency is at 10KHz to 20KHz, and one cycle time is 100μs for a 10KHz of PWM frequency. In current shunt monitoring for a motor phase, the phase current is converted to a phase voltage signal for ADC sampling. This sampling voltage signal must be settled before entering the ADC. As the Figure 19 shown, the total settling time of a current shunt monitor circuit includes: the rising edge delay time (t_{SR}) due to the op-amp's slew rate, and the measurement settling time (t_{SET}). For a 2-shunt solution of motor phase current sensing, if the minimum duty cycle of the PWM is defined at 5%, and the t_{SR} is required at 20% of a total time window for a phase current monitoring, in case of a 3.3V motor control system (3.3V MCU with 12-bit ADC), the op-amp's slew rate should be more than:

$$\frac{3.3V}{100us \times 5\% \times 20\%} = 3.3V / us \quad (2)$$

At the same time, the op-amp's bandwidth should be much greater than the PWM frequency, like 10 time at least.

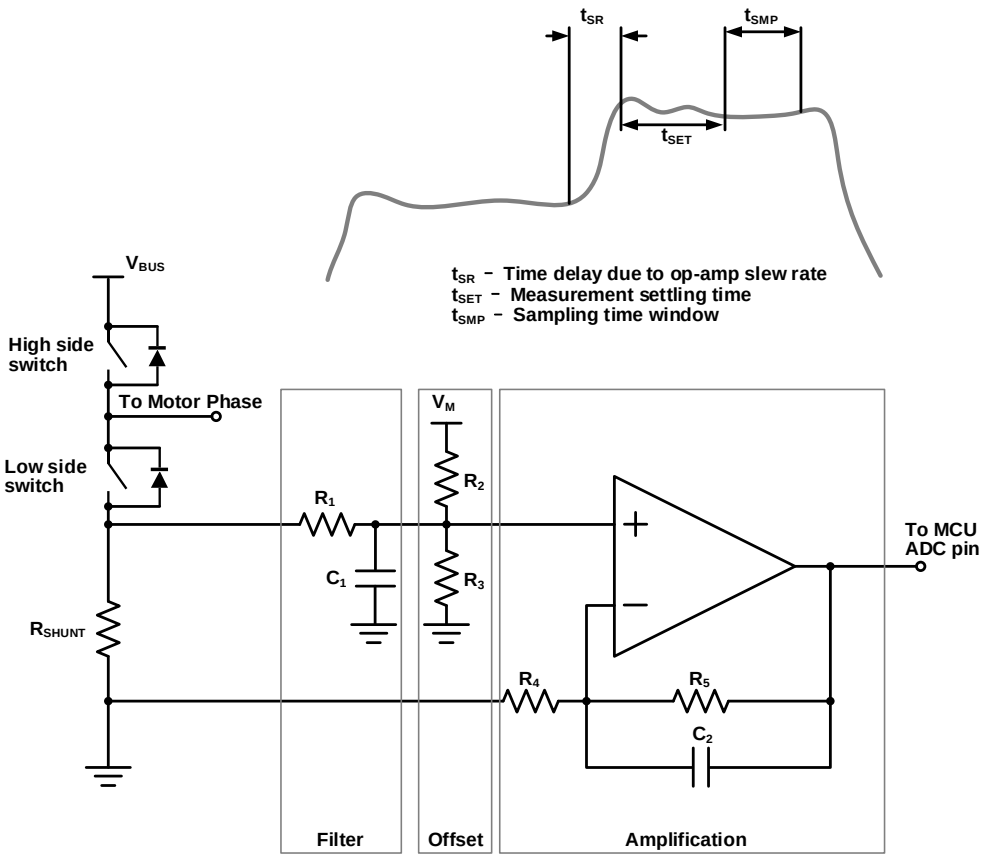


Figure 19. Current Shunt Monitor Circuit

7.1.3 Differential Amplifier

The circuit shown in Figure 20 performs the difference function. If the resistors ratios are equal R4/R3 = R2/R1, then:

$$V_{OUT} = (V_P - V_N) \times \frac{R_2}{R_1} + V_{REF} \quad (3)$$

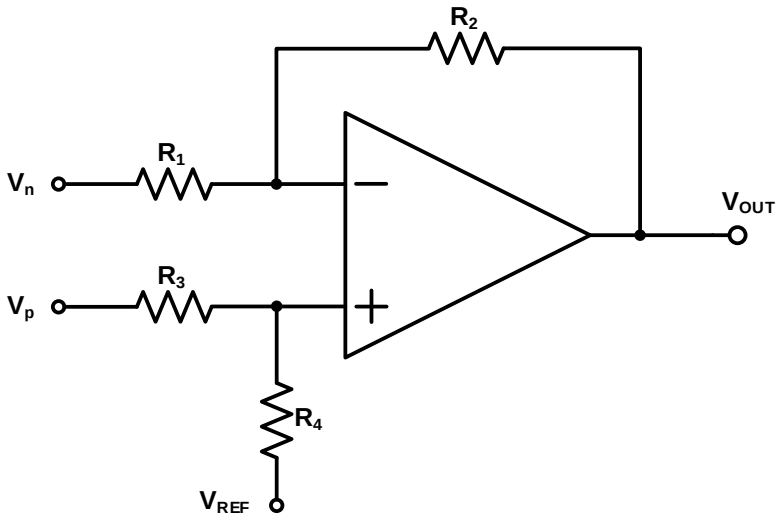


Figure 20. Differential Amplifier

7.1.4 Instrumentation Amplifier

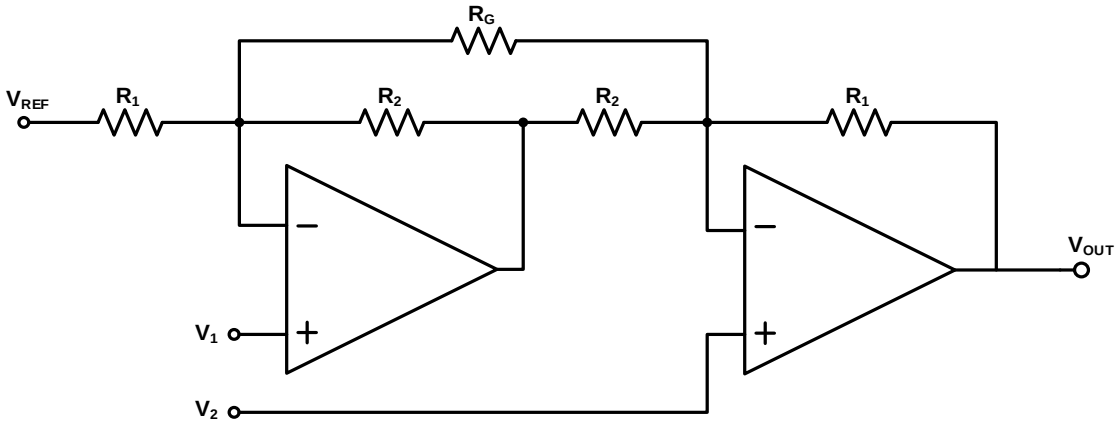


Figure 21. Instrumentation Amplifier

The GD30AP863x family is well suited for conditioning sensor signals in battery-powered applications. Figure 21 shows a two op-amp instrumentation amplifier, using the GD30AP863x op-amps. The circuit works well for applications requiring rejection of common-mode noise at higher gains. The reference voltage (V_{REF}) is supplied by a low-impedance source. In single voltage supply applications, the V_{REF} is typically $V_S/2$.

$$V_{OUT} = (V_1 - V_2) \times \left(1 + \frac{R_1}{R_2} + \frac{2R_1}{R_G}\right) + V_{REF} \quad (4)$$

7.1.5 Buffered Chemical Sensors

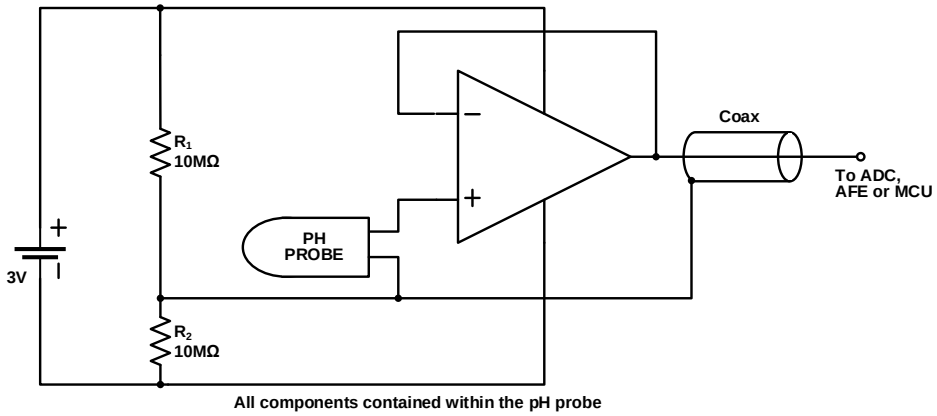


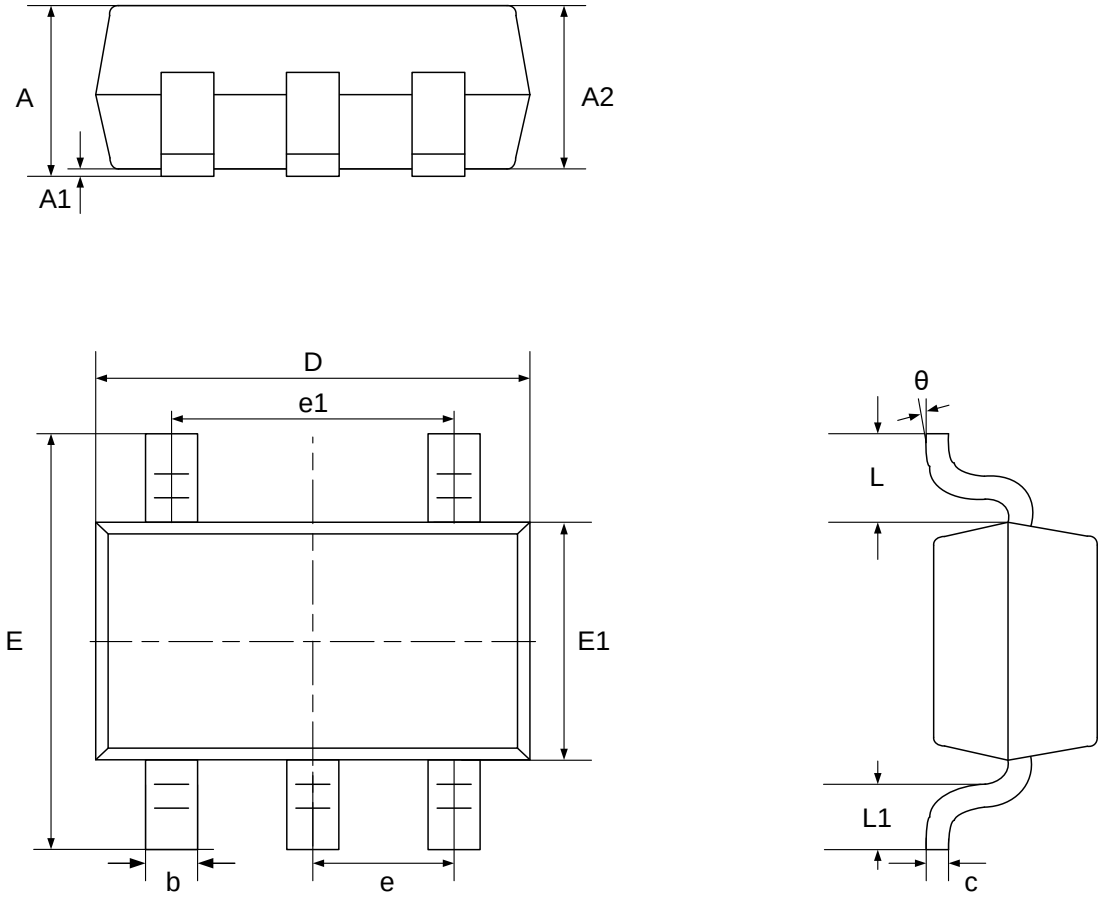
Figure 22. Buffered pH Probe

The GD30AP863x family has input bias current in the pA range. This is ideal in buffering high impedance chemical sensors, such as pH probes. As an example, the circuit in Figure 22 eliminates expansive low-leakage cables that is required to connect a pH probe (general purpose combination pH probes, e.g Corning 476540) to metering ICs such as ADC, AFE and/or MCU. A GD30AP863x op-amp and a lithium battery are housed in the probe assembly. A conventional low-cost coaxial cable can be used to carry the op-amp's output signal to subsequent ICs for pH reading.

8 Package Information

8.1 Outline Dimensions

SOT23-5L Package Outline



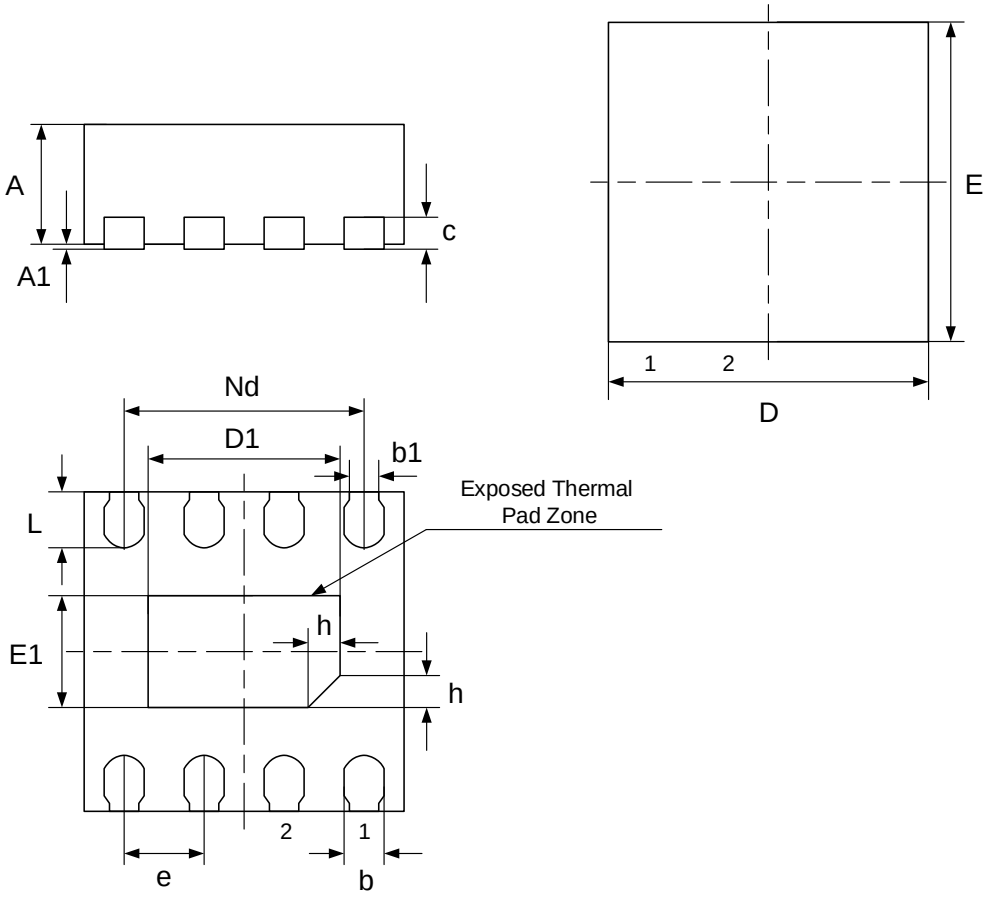
NOTES:

1. All dimensions are in millimeters.
2. Package dimensions does not include mold flash, protrusions, or gate burrs.
3. Refer to the Table 1 *SOT23-5L dimensions(mm)*.

Table 1. SOT23-5L dimensions(mm)

SYMBOL	MIN	TYP	MAX
A			1.35
A1	0.00		0.15
A2	1.00		1.20
b	0.35		0.45
c	0.14		0.20
D	2.82		3.02
E	2.60		3.00
E1	1.526		1.726
e	0.95 BSC		
e1	1.90 BSC		
L	0.60 REF		
L1	0.30		0.60
θ	0°		8°

DFN2x2-8L Package Outline



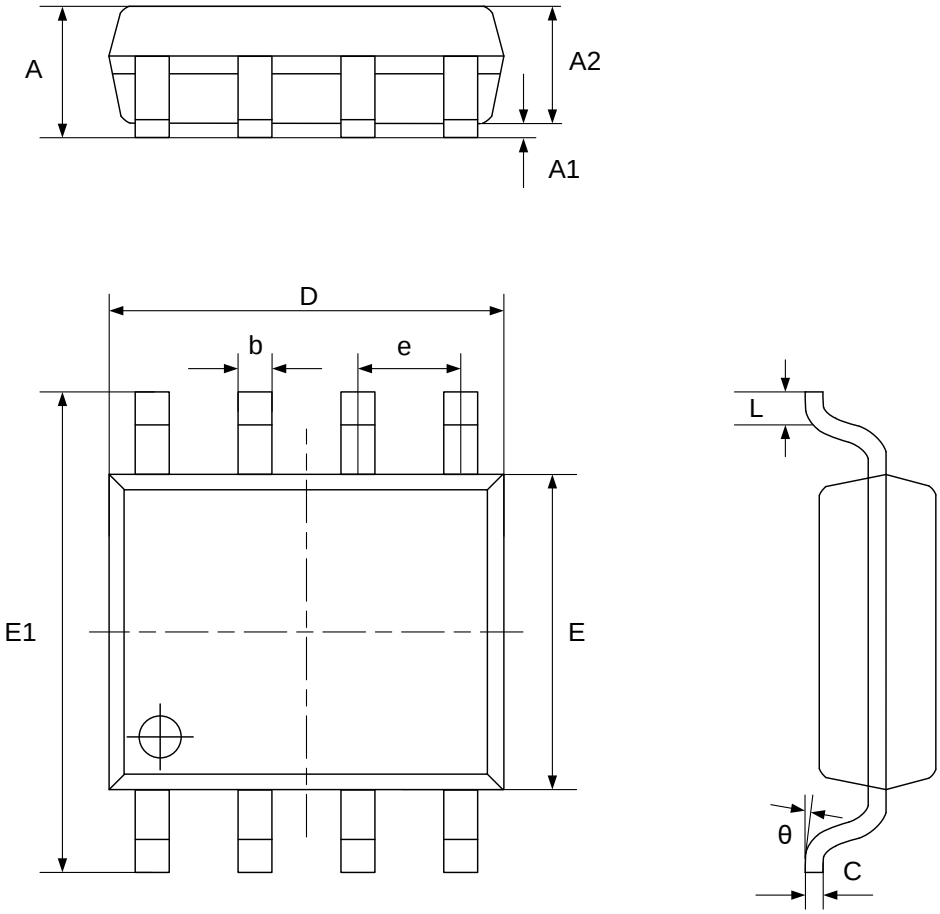
NOTES: (continued)

1. Refer to the Table 2 *DFN2x2-8L dimensions(mm).*

Table 2. DFN2x2-8L dimensions(mm)

SYMBOL	MIN	TYP	MAX
A	0.70	0.75	0.80
A1		0.02	0.05
b	0.20	0.25	0.30
b1		0.18 REF	
c	0.18	0.20	0.25
D	1.90	2.00	1.30
D1	1.10	1.20	1.30
Nd		1.50 BSC	
E	1.90	2.00	2.10
E1	0.60	0.70	0.80
e		0.50 BSC	
L	0.30	0.35	0.40
h	0.15	0.20	0.25

SOIC-8L Package Outline



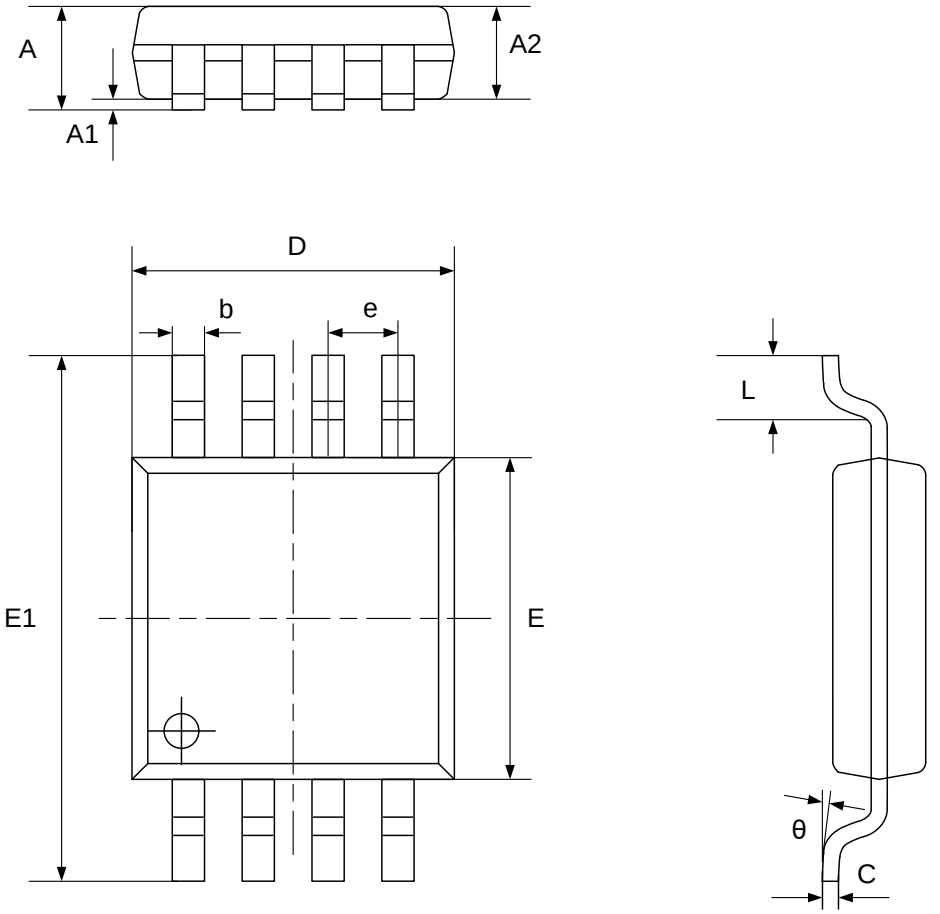
NOTES: (continued)

1. Refer to the Table 3 *SOIC-8L dimensions(mm)*.

Table 3. SOIC-8L dimensions(mm)

SYMBOL	MIN	TYP	MAX
A	1.370		1.670
A1	0.070		0.170
A2	1.300		1.500
b	0.306		0.506
C		0.203	
D	4.700		5.100
E	3.820		4.020
E1	5.800		6.200
e		1.270	
L	0.450		0.750
θ	0°		8°

MSOP-8L Package Outline



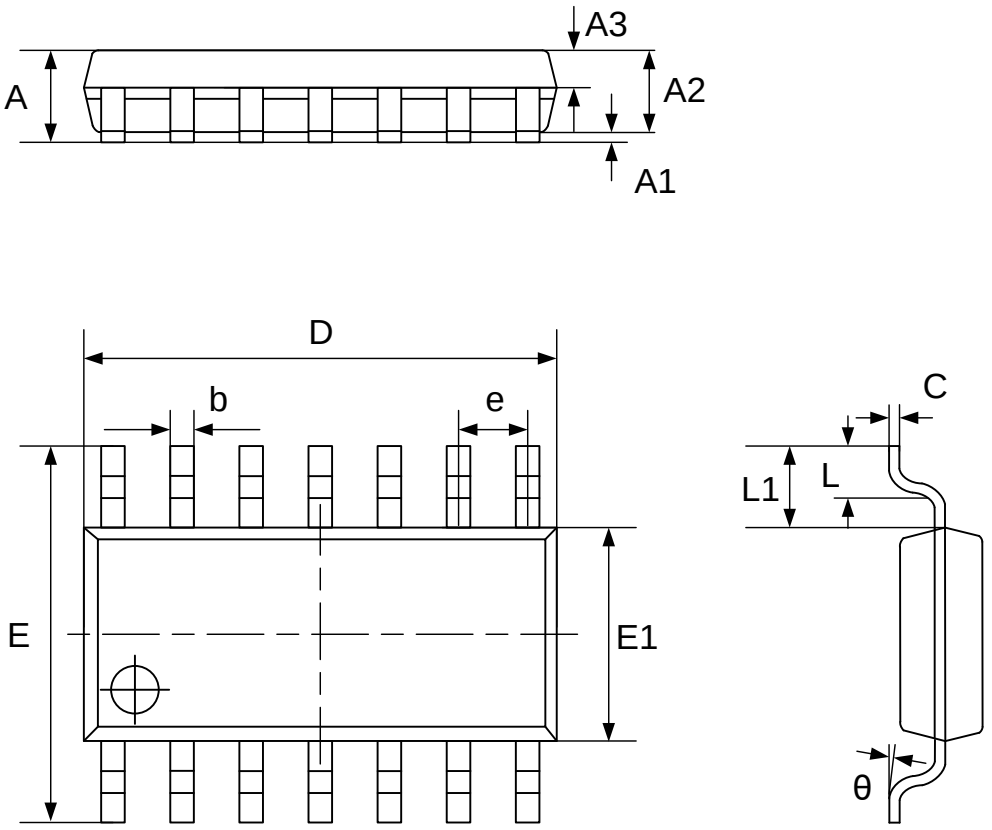
NOTES: (continued)

1. Refer to the Table 4 *MSOP-8L dimensions(mm)*.

Table 4. MSOP-8L dimensions(mm)

SYMBOL	MIN	TYP	MAX
A	0.800		1.100
A1	0.050		0.150
A2	0.750		0.950
b	0.290		0.380
C	0.150		0.200
D	2.900		3.100
E	2.900		3.100
E1	4.700		5.100
e		0.650	
L	0.400		0.700
θ	0°		8°

SOIC-14L Package Outline



NOTES: (continued)

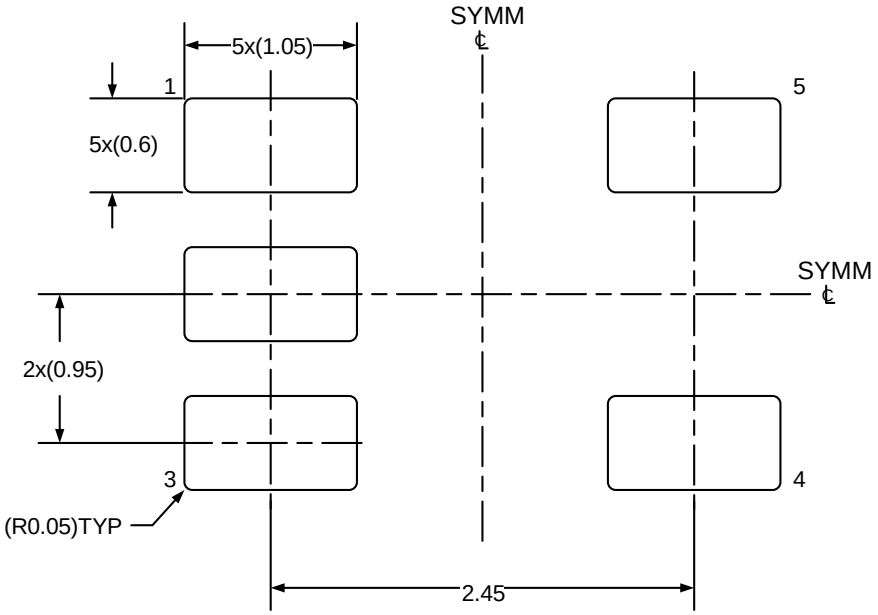
1. Refer to the Table 5 *SOIC-14L dimensions(mm)*.

Table 5. SOIC-14L dimensions(mm)

SYMBOL	MIN	TYP	MAX
A	1.450		1.850
A1	0.100		0.300
A2	1.350		1.550
A3	0.550		0.750
b		0.406	
C		0.203	
D	8.630		8.830
E	5.840		6.240
E1	3.850		4.050
e		1.270	
L1	1.040 REF		
L	0.350		0.750
θ	2°		8°

8.2 Recommended Land Pattern

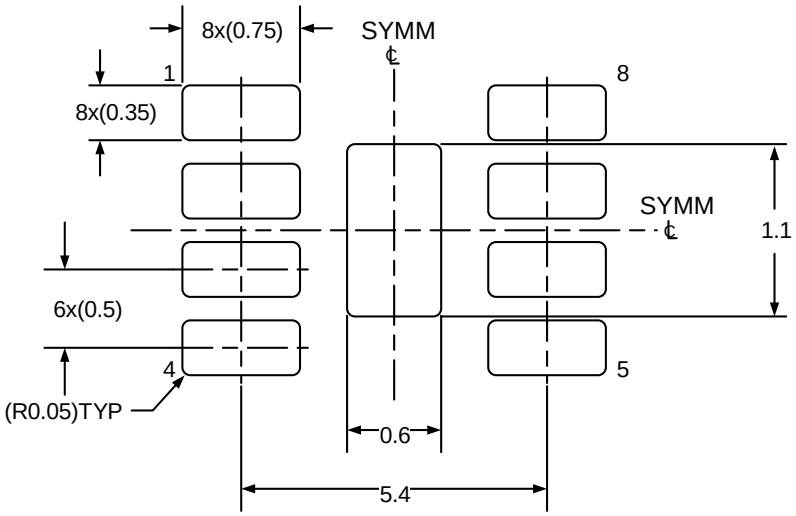
SOT23-5L Land Pattern Example



NOTES: (continued)

1. Refer to the IPC-7351 can also help you complete the designs.
2. Exposed metal shown.
3. Drawing is 20X scale.

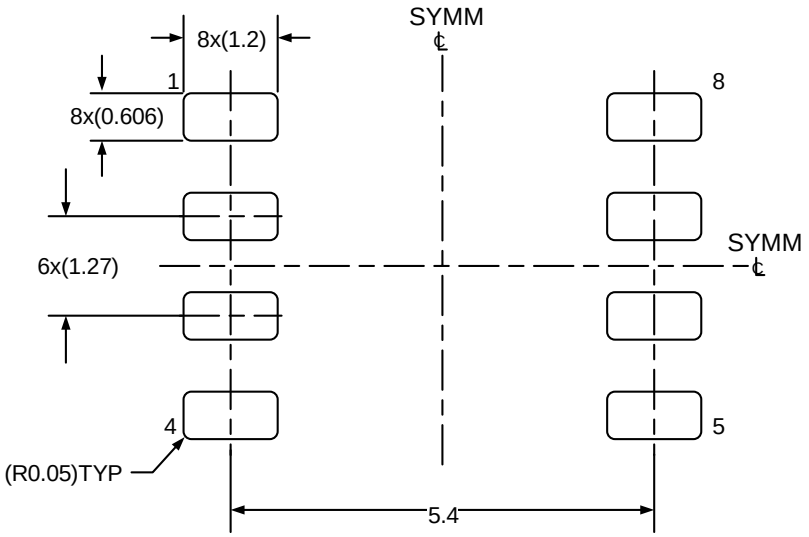
DFN2x2-8L Land Pattern Example



NOTES: (continued)

1. Refer to the IPC-7351 can also help you complete the designs.
2. Exposed metal shown.
3. Drawing is 20X scale.

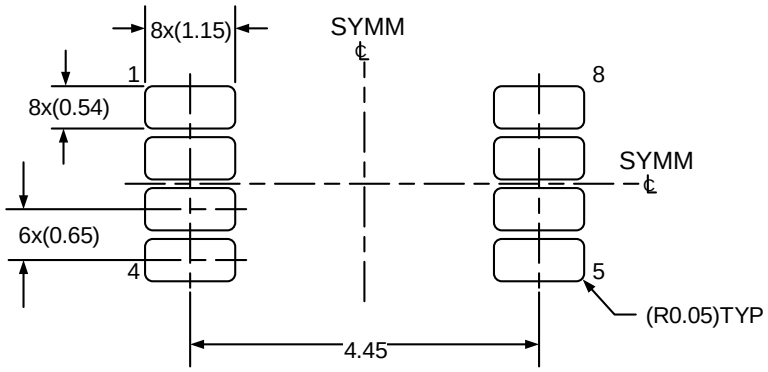
SOIC-8L Land Pattern Example



NOTES: (continued)

1. Refer to the IPC-7351 can also help you complete the designs.
2. Exposed metal shown.
3. Drawing is 10X scale.

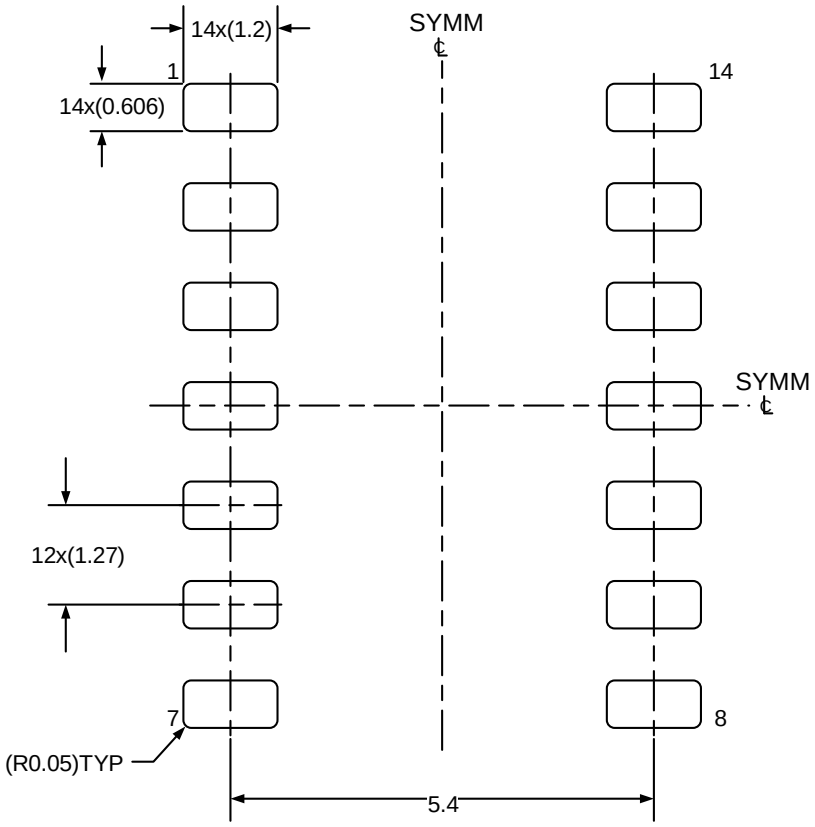
MSOP-8L Land Pattern Example



NOTES: (continued)

1. Refer to the IPC-7351 can also help you complete the designs.
2. Exposed metal shown.
3. Drawing is 10X scale.

SOIC-14L Land Pattern Example



NOTES: (continued)

1. Refer to the IPC-7351 can also help you complete the designs.
2. Exposed metal shown.
3. Drawing is 10X scale.

9 Ordering Information

Ordering Code	Package Type	ECO Plan	Packing Type	MOQ	OP Temp(°C)
GD30AP8631NSTR-I01	SOT23-5L	Green	Tape & Reel	3000	−40°C to +125°C
GD30AP8632WETR-I02	DFN2x2-8L	Green	Tape & Reel	3000	−40°C to +125°C
GD30AP8632WLTR-I02	SOIC-8L	Green	Tape & Reel	4000	−40°C to +125°C
GD30AP8632WMTR-I02	MSOP-8L	Green	Tape & Reel	3000	−40°C to +125°C
GD30AP8634ZLTR-I04	SOIC-14L	Green	Tape & Reel	2500	−40°C to +125°C

10 Revision History

REVISION NUMBER	DESCRIPTION	DATE
1.0	Initial release and device details	2024

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